



Ferrites and accessories

General – Definitions

Date: October 2022

1 Hysteresis

The special feature of ferromagnetic and ferrimagnetic materials is that spontaneous magnetization sets in below a material-specific temperature (Curie point). The elementary atomic magnets are then aligned in parallel within macroscopic regions. These so-called Weiss' domains are normally oriented so that no magnetic effect is perceptible. But it is different when a ferromagnetic body is placed in a magnetic field and the flux density B as a function of the magnetic field strength H is measured with the aid of a test coil. Proceeding from H = 0 and B = 0, the so-called initial magnetization curve is first obtained. At low levels of field strength, those domains that are favorably oriented to the magnetic field grow at the expense of those that are not. This produces what are called wall displacements. At higher field strength, whole domains overturn magnetically – this is the steepest part of the curve – and finally the magnetic moments are moved out of the preferred states given by the crystal lattice into the direction of the field until saturation is obtained, i.e. until all elementary magnets in the material are in the direction of the field. If H is now reduced again, the B curve is completely different. The relationship shown in the hysteresis loop (figure 1) is obtained.

1.1 Hysteresis loop

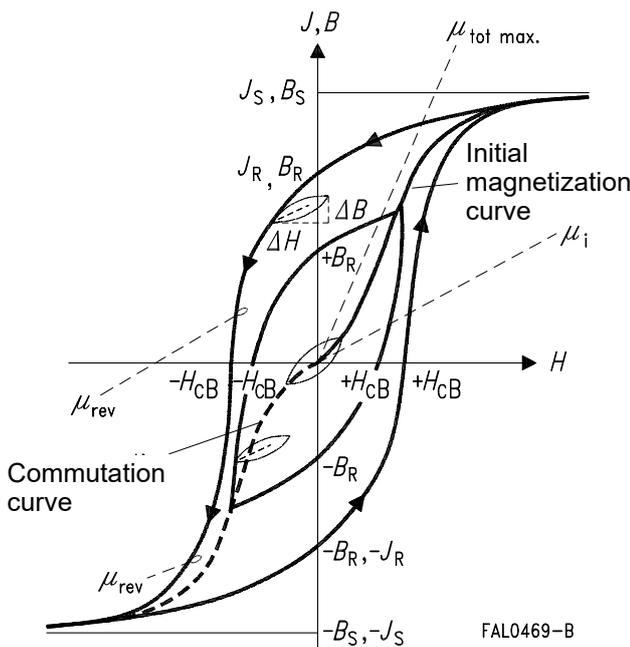


Figure 1
Magnetization curve
(schematic)

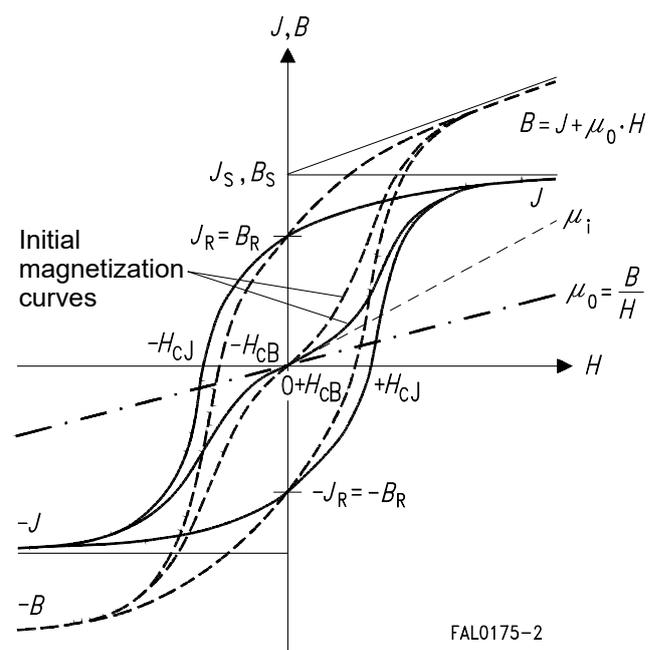


Figure 2
Hysteresis loops for different
excitations and materials

Magnetic field strength $H = \frac{I \cdot N}{l} = \frac{\text{ampere-turns}}{\text{length in m}} \quad \left[\frac{\text{A}}{\text{m}} \right]$

Magnetic flux density $B = \frac{\Phi}{A} = \frac{\text{magnetic flux}}{\text{permeated area}} \quad \left[\frac{\text{Vs}}{\text{m}^2} \right] = [\text{T(Tesla)}]$

Polarization J $J = B - \mu_0 H \quad \mu_0 \cdot H \ll J \Rightarrow B \approx J$

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General relationship between B and H:

$$B = \mu_0 \cdot \mu_r(H) \cdot H$$

μ_0 Magnetic field constant
 μ_0 $1.257 \cdot 10^{-6} \left[\frac{\text{Vs}}{\text{Am}} \right]$
 μ_r Relative permeability

In a vacuum, $\mu_r = 1$; in ferromagnetic or ferrimagnetic materials the relation B(H) becomes nonlinear and the slope of the hysteresis loop $\mu_r \gg 1$.

1.2 Basic parameters of the hysteresis loop

1.2.1 Initial magnetization curve

The initial magnetization curve describes the relationship $B = \mu_r \mu_0 H$ for the first magnetization following a complete demagnetization. By joining the end points of all “sub-loops”, from $H = 0$ to $H = H_{\text{max}}$, (as shown in figure 1), we obtain the so-called commutation curve (also termed normal or mean magnetization curve), which, for magnetically soft ferrite materials, coincides with the initial magnetization curve.

1.2.2 Saturation magnetization B_S

The saturation magnetization B_S is defined as the maximum flux density attainable in a material (i.e. for a very high field strength) at a given temperature; above this value B_S , it is not possible to further increase B(H) by further increasing H.

Technically, B_S is defined as the flux density at a field strength of $H = 1200 \text{ A/m}$. As is confirmed in the actual magnetization curves in the chapter on “Materials”, the B(H) characteristic above 1200 A/m remains roughly constant (applies to all ferrites with high initial permeability, i.e. where $\mu \geq 1000$).

1.2.3 Remanent flux density $B_R(H)$

The remanent flux density (residual magnetization density) is a measure of the degree of residual magnetization in the ferrite after traversing a hysteresis loop. If the magnetic field H is subsequently reduced to zero, the ferrite still has a material-specific flux density $B_R \neq 0$ (see figure 1: intersection with the ordinate $H = 0$).

1.2.4 Coercive field strength H_C

The flux density B can be reduced to zero again by applying a specific opposing field $-H_C$ (see figure 1: intersection with the abscissa $B = 0$).

The demagnetized state can be restored at any time by:

- traversing the hysteresis loop at a high frequency and simultaneously reducing the field strength H to $H = 0$.
- by exceeding the Curie temperature T_C .

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2 Permeability

Different relative permeabilities μ are defined on the basis of the hysteresis loop for the various electromagnetic applications.

2.1 Initial permeability μ_i

$$\mu_i = \frac{1}{\mu_0} \cdot \frac{\Delta B}{\Delta H} \quad (\Delta H \rightarrow 0)$$

The initial permeability μ_i defines the relative permeability at very low excitation levels and constitutes the most important means of comparison for soft magnetic materials. According to IEC 60401-3, μ_i is defined using closed magnetic circuits (e.g. a closed ring-shaped cylindrical coil) for $f \leq 10$ kHz, $B < 0.25$ mT, $T = 25$ °C.

2.2 Effective permeability μ_e

Most core shapes in use today do not have closed magnetic paths (only ring, double E or double-aperture cores have closed magnetic circuits), rather the circuit consists of regions where $\mu_i \neq 1$ (ferrite material) and $\mu_i = 1$ (air gap). Figure 3 shows the shape of the hysteresis loop of a circuit of this type.

In practice, an effective permeability μ_e is defined for cores with air gaps.

$$\mu_e = \frac{1}{\mu_0 N^2} \sum \frac{L}{A}$$

$\sum \frac{L}{A}$ Form factor
 L Inductance
 N Number of turns

It should be noted, for example, that the loss factor $\tan \delta$ and the temperature coefficient for gapped cores reduce in the ratio μ_e/μ_i compared to ungapped cores.

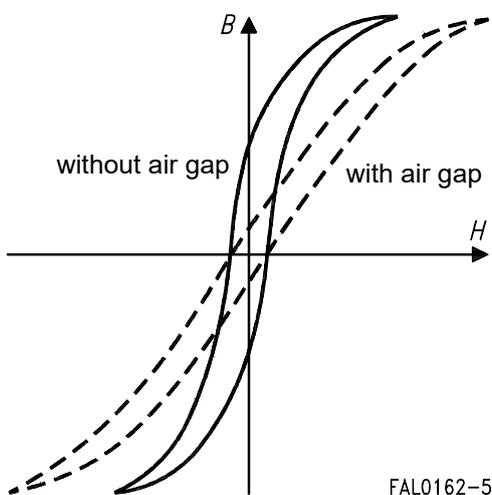


Figure 3
Comparison of hysteresis loops for a core with and without an air gap

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The following approximation applies for an air gap $s \ll l_e$:

$$\mu_e = \frac{\mu_i}{1 + \frac{s}{l_e} \cdot \mu_i}$$

s Width of air gap

l_e Effective magnetic path length

For more precise calculation methods, see for example E.C. Snelling, "Soft ferrites", 2nd edition.

2.3 Apparent permeability μ_{app}

$$\mu_{app} = \frac{L}{L_0} = \frac{\text{inductance with core}}{\text{inductance without core}}$$

The definition of μ_{app} is particularly important for specification of the permeability for coils with tubular, cylindrical and threaded cores, since an unambiguous relationship between initial permeability μ_i and effective permeability μ_e is not possible on account of the high leakage inductances. The design of the winding and the spatial correlation between coil and core have a considerable influence on μ_{app} . A precise specification of μ_{app} requires a precise specification of the measuring coil arrangement.

2.4 Complex permeability $\bar{\mu}$

To enable a better comparison of ferrite materials and their frequency characteristics at very low field strengths (in order to take into consideration the phase displacement between voltage and current), it is useful to introduce μ as a complex operator, i.e. a complex permeability $\bar{\mu}$, according to the following relationship:

$$\bar{\mu} = \mu_s' - j \cdot \mu_s''$$

where, in terms of a series equivalent circuit, (see figure 5)

μ_s' is the relative real (inductance) component of $\bar{\mu}$

and μ_s'' is the relative imaginary (loss) component of $\bar{\mu}$.

Using the complex permeability $\bar{\mu}$, the (complex) impedance of the coil can be calculated:

$$\bar{Z} = j \omega \bar{\mu} L_0$$

where L_0 represents the inductance of a core of permeability $\mu_r = 1$, but with unchanged flux distribution.

(cf. also section 4.1: information on $\tan \delta$)

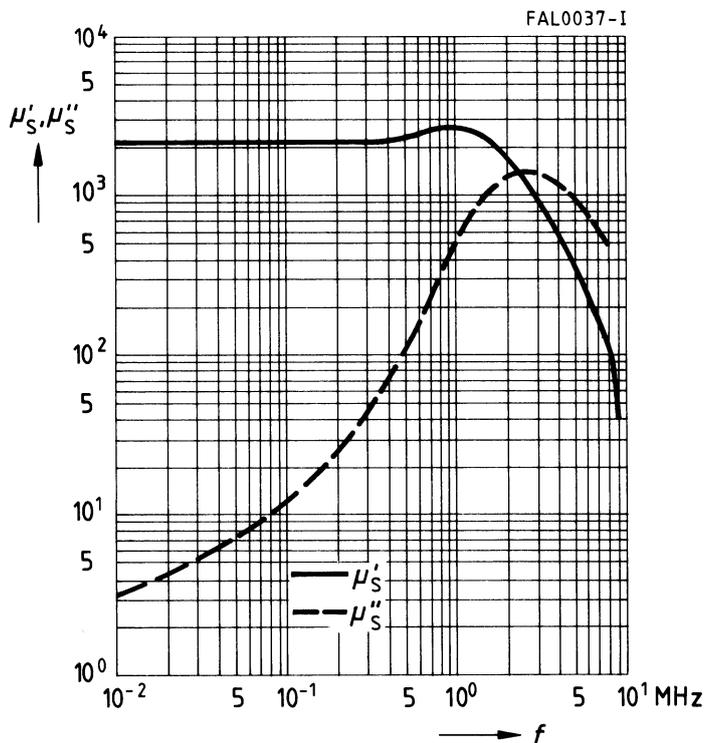


Figure 4
Complex permeability versus frequency
(measured on R10 toroids, N48 material, measuring flux density $\hat{B} \leq 0.25$ mT)

Figure 4 shows the characteristic shape of the curves of μ'_s and μ''_s as functions of the frequency, using N48 material as an example. The real component μ'_s is constant at low frequencies, attains a maximum at higher frequencies and then drops in approximately inverse proportion to f . At the same time, μ''_s rises steeply from a very small value at low frequencies to attain a distinct maximum and, past this, also drops as the frequency is further increased.

The region in which μ' decreases sharply and where the μ'' maximum occurs is termed the cut-off frequency f_{cutoff} . This is inversely proportional to the initial permeability of the material (Snoek's law).

2.5 Reversible permeability μ_{rev}

$$\mu_{\text{rev}} = \frac{1}{\mu_0} \cdot \lim_{\Delta H \rightarrow 0} \left(\frac{\Delta B}{\Delta H} \right)_{H_{\text{DC}}} \quad (\text{Permeability with superimposed DC field } H_{\text{DC}})$$

In order to measure the reversible permeability μ_{rev} , a small measuring alternating field is superimposed on a DC field. In this case μ_{rev} is heavily dependent on H_{DC} , the core geometry and the temperature.

Important application areas for DC field-superimposed, i.e. magnetically biased coils are broadband transformer systems (feeding currents with signal superimposition) and power engineering (shifting the operating point) and the area known as "nonlinear chokes" (cf. chapter on RM cores). For the magnetic bias curves as a function of the excitation H_{DC} see the chapter on "SIFERRIT materials".

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2.6 Amplitude permeability μ_a , A_{L1} value

$$\mu_a = \frac{\hat{B}}{\mu_0 \hat{H}} \quad (\text{Permeability at high excitation})$$

\hat{B} Peak value of flux density

\hat{H} Peak value of field strength

For frequencies well below cut-off frequency, μ_a is not frequency-dependent but there is a strong dependence on temperature. The amplitude permeability is an important definition quantity for power ferrites. It is defined for specific core types by means of an A_{L1} value for $f \leq 10$ kHz, $B = 320$ mT (or 200 mT), $T = 100$ °C.

$$A_{L1} = \frac{\mu_0 \cdot \mu_a}{\sum \frac{l}{A}}$$

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3 Magnetic core shape characteristics

Permeabilities and also other magnetic parameters are generally defined as material-specific quantities. For a particular core shape, however, the magnetic data are influenced to a significant extent by the geometry. Thus, the inductance of a slim-line ring core coil is defined as:

$$L = \mu_r \cdot \mu_0 \cdot N^2 \cdot \frac{A}{l}$$

Due to their geometry, soft magnetic ferrite cores in the field of such a coil change the flux parameters in such a way that it is necessary to specify a series of effective core shape parameters in each data sheet. The following are defined:

l_e	Effective magnetic length
A_e	Effective magnetic cross section
A_{\min}	Min. magnetic cross section of the core (required to calculate the max. flux density)
$V_e = A_e \cdot l_e$	Effective magnetic volume

With the aid of these parameters, the calculation for ferrite cores with complicated shapes can be reduced to the considerably more simple problem of an imaginary ring core with the same magnetic properties. The basis for this is provided by the methods of calculation according to IEC 60205, which allow to calculate the effective core shape parameters of different core shapes.

3.1 Form factor

$$\sum \frac{l}{A} = \frac{l_e}{A_e}$$

The inductance L can then be calculated as follows:

$$L = \frac{\mu_e \cdot \mu_0 \cdot N^2}{\sum \frac{l}{A}}$$

where μ_e denotes the effective permeability or another permeability μ_{rev} or μ_a (or μ_i for cores with a closed magnetic path) adapted for the B/H range in question.

3.2 Inductance factor, A_L value

$$A_L = \frac{L}{N^2} = \frac{\mu_e \cdot \mu_0}{\sum \frac{l}{A}}$$

A_L is the inductance referred to number of turns = 1. Therefore, for a defined number of turns N :

$$L = A_L \cdot N^2$$

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3.3 Tolerance code letters

The tolerances of the A_L are coded by the letters in the third block of the ordering code in conformity with IEC 62358.

Code letter	Tolerance of A_L value	Code letter	Tolerance of A_L value
A	$\pm 3\%$	L	$\pm 15\%$
B	$\pm 4\%$	M	$\pm 20\%$
C	$\pm 6\%$	Q	+30/-10%
D	$\pm 8\%$	R	+30/-20%
E	$\pm 7\%$	U	+80/-0%
H	$\pm 12\%$	X	filling letter
J	$\pm 5\%$	Y	+40/-30%
K	$\pm 10\%$		

The tolerance values available are given in the individual data sheets.

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4 Definition quantities in the small-signal range

4.1 Loss factor $\tan \delta$

Losses in the small-signal range are specified by the loss factor $\tan \delta$.

Based on the impedance \bar{Z} (cf. also section 2.4), the loss factor of the core in conjunction with the complex permeability $\bar{\mu}$ is defined as

$$\tan \delta_s = \frac{\mu_s''}{\mu_s'} = \frac{R_s}{\omega L_s} \quad \text{and} \quad \tan \delta_p = \frac{\mu_p''}{\mu_p'} = \frac{\omega \cdot L_p}{R_p}$$

where R_s and R_p denote the series and parallel resistance and L_s and L_p the series and parallel inductance respectively.

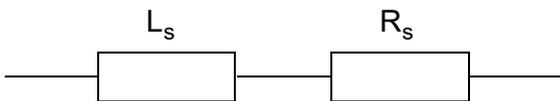


Figure 5
Lossless series inductance L_s with loss resistance R_s resulting from the core losses.

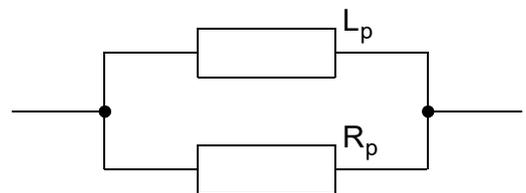


Figure 6
Lossless parallel inductance L_p with loss resistance R_p resulting from the core losses.

From the relationships between series and parallel circuits we obtain:

$$\mu_p' = \mu_s' \cdot (1 + (\tan \delta)^2)$$

$$\mu_p'' = \mu_s'' \cdot \left(1 + \left(\frac{1}{\tan \delta}\right)^2\right)$$

4.2 Relative loss factor $\tan \delta / \mu_i$

In gapped cores the material loss factor $\tan \delta$ is reduced by the factor μ_e / μ_i . This results in the relative loss factor $\tan \delta_e$ (cf. also section 2.2):

$$\tan \delta_e = \frac{\tan \delta}{\mu_i} \cdot \mu_e$$

The table of material properties lists the relative loss factor $\tan \delta / \mu_i$. This is determined to IEC 60401-3 at $B = 0.25 \text{ mT}$, $T = 25 \text{ }^\circ\text{C}$.

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4.3 Quality factor Q

The ratio of reactance to total resistance of an induction coil is known as the quality factor Q.

$$Q = \frac{\omega L}{R_L} = \frac{\text{reactance}}{\text{total resistance}}$$

The total quality factor Q is the reciprocal of the total loss factor $\tan \delta$ of the coil; it is dependent on the frequency, inductance, temperature, winding wire and permeability of the core.

4.4 Hysteresis loss resistance R_h and hysteresis material constant η_B

In transformers, in particular, the user cannot always be content with very low saturation. The user requires details of the losses which occur at higher saturation, e.g. where the hysteresis loop begins to open.

Since this hysteresis loss resistance R_h can rise sharply in different flux density ranges and at different frequencies, it is measured to IEC 60401-3 for μ_i values greater than 500 at $B_1 = 1.5$ and $B_2 = 3$ mT ($\Delta B = 1.5$ mT), a frequency of 10 kHz and a temperature of 25 °C (for $\mu_i < 500$: $f = 100$ kHz, $B_1 = 0.3$ mT, $B_2 = 1.2$ mT). The hysteresis loss factor $\tan \delta_h$ can then be calculated from this.

$$\tan \delta_h = \frac{R_h}{\omega \cdot L} = \tan \delta(B_2) - \tan \delta(B_1)$$

For the hysteresis material constant η_B we obtain:

$$\eta_B = \frac{\tan \delta_h}{\mu_e \cdot \Delta \hat{B}}$$

The hysteresis material constant, η_B , characterizes the material-specific hysteresis losses and is a quantity independent of the air gap in a magnetic circuit.

The hysteresis loss factor of an inductor can be reduced, at a constant flux density, by means of an (additional) air gap

$$\tan \delta_h = \eta_B \cdot \Delta \hat{B} \cdot \mu_e$$

For further details on the measurement techniques see IEC 62044-2.

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5 Definition quantities in the high-excitation range

While in the small-signal range ($H \leq H_c$), i.e. in filter and broadband applications, the hysteresis loop is generally traversed only in lancet form (figure 2), for power applications the hysteresis loop is driven partly into saturation. The defining quantities are then

μ_{rev} = reversible permeability in the case of superimposition with a DC signal
(operating point for power transformers)

μ_a = amplitude permeability and

P_V = core losses.

5.1 Core losses P_V

The losses of a ferrite core or core set P_V is proportional to the area of the hysteresis loop in question. It can be divided into three components:

$$P_V = P_{V, \text{ hysteresis}} + P_{V, \text{ eddycurrent}} + P_{V, \text{ residual}}$$

Owing to the high specific resistance of ferrite materials, the eddy current losses in the frequency range common today (1 kHz to 2 MHz) may be practically disregarded except in the case of core shapes having a large cross-sectional area.

The power loss P_V is a function of the temperature T , the frequency f , the flux density B and is of course dependent on ferrite material and core shape.

The temperature dependence can generally be approximated by means of a third-order polynomial, while

$$P_V(f) \sim f^{(1+x)} \quad 0 \leq x \leq 1$$

applies for the frequency dependence and

$$P_V(B) \sim B^{(2+y)} \quad 0 \leq y \leq 1$$

for the flux density dependence. The coefficients x and y are dependent on core shape and material, and there is a mutual dependence between the coefficients of the definition quantity (e.g. T) and the relevant parameter set (e.g. f , B).

In the case of cores which are suitable for power applications, the total core losses P_V are given explicitly for a specific frequency f , flux density B and temperature T in the relevant data sheets.

When determining the total power loss for an inductive component, the winding losses must also be taken into consideration in addition to the core-specific losses.

$$P_{V, \text{ tot}} = P_{V, \text{ core}} + P_{V, \text{ winding}}$$

where, in addition to insulation conditions in the given frequency range, skin effect and proximity effect must also be taken into consideration for the winding.

5.2 Performance factor ($PF = f \cdot B_{\max}$)

The performance factor is a measure of the maximum power which a ferrite can transmit, whereby it is generally assumed that the loss does not exceed 300 kW/m³. Heat dissipation values of this order are usually assumed when designing small and medium-sized transformers. Increasing the performance factor will either enable an increase of the power that can be transformed by a core of identical design, or a reduction in component size if the transformed power is not increased.

If the performance factors of different power transformer materials are plotted as a function of frequency, only slight differences are observed at low frequencies (<300 kHz), but these differences become more pronounced with increasing frequency. This diagram can be used to determine the optimum material for a given frequency range.

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6 Influence of temperature

6.1 $\mu(T)$ curve, Curie temperature T_C

The initial permeability μ_i as a function of T is given for all materials (see chapter on SIFERRIT materials). Important parameters for a $\mu(T)$ curve are the position of the **secondary permeability maximum** (SPM) and the Curie temperature. Minimum losses occur at the SPM temperature.

Above the Curie temperature T_C ferrite materials lose their ferrimagnetic properties, i.e. μ_i drops to $\mu_i = 1$. This means that the parallel alignment of the elementary magnets (spontaneous magnetization) is destroyed by increasing thermal activation. This phenomenon is reversible, i.e. when the temperature is reduced below T_C again, the ferrimagnetic properties are restored.

The Curie temperature T_C is defined as the cross of the straight line between 80% and 20% of L_{max} with the temperature axes (figure 7).

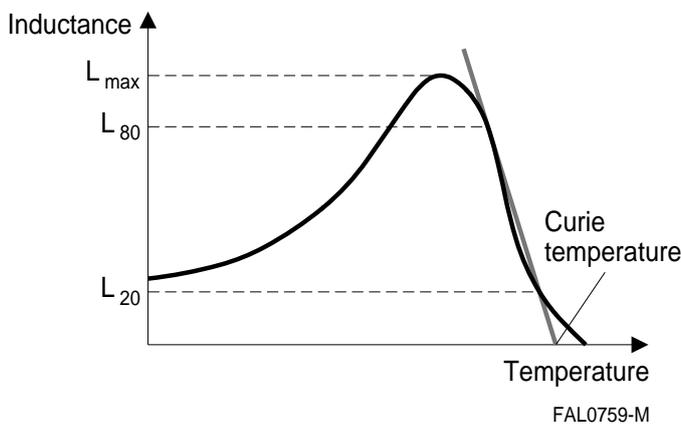


Figure 7
Definition of Curie temperature

6.2 Temperature coefficient of permeability α

By definition the temperature coefficient α represents a straight line of average gradient between the reference temperatures T_1 and T_2 . If the $\mu(T)$ curve is approximately linear in this temperature range, this is a good approximation; in the case of heavily pronounced maxima, as occur particularly with highly permeable broadband ferrites, however, this is less true. The following applies:

$$\alpha = \frac{\mu_{i2} - \mu_{i1}}{\mu_{i1}} \cdot \frac{1}{T_2 - T_1}$$

μ_{i1} Initial permeability μ_i at $T_1 = 25\text{ °C}$

μ_{i2} The initial permeability μ_i associated with the temperature T_2

6.3 Relative temperature coefficient α_F

$$\alpha_F = \frac{\alpha}{\mu_i} = \frac{\mu_{i2} - \mu_{i1}}{\mu_{i2} \cdot \mu_{i1}} \cdot \frac{1}{T_2 - T_1}$$

In a magnetic circuit with an air gap and the effective permeability μ_e the temperature coefficient is reduced by the factor μ_e/μ_i (cf. also section 2.2).

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6.4 Permeability factor

The first factor in the equation for determining the relative temperature coefficient $\frac{\mu_{i2} - \mu_{i1}}{\mu_{i2} \cdot \mu_{i1}}$ is known as the permeability factor.

In the case of SIFERRIT materials for resonant circuits, the temperature dependence of the permeability factor can be seen from the relevant diagram.

6.5 Effective temperature coefficient α_e

$$\alpha_e = \frac{\mu_e}{\mu_i} \cdot \alpha$$

In the case of the ferrite materials for filter applications, the α/μ_i values for the ranges 25 to 55 °C and 5 to 25 °C are given in the table of material properties.

The effective permeability μ_e is required in order to calculate α_e ; therefore this is given for each core in the individual data sheets.

6.6 Relationship between the change in inductance and the permeability factor

The relative change in inductance between two temperature points can be calculated as follows:

$$\frac{L_2 - L_1}{L_1} = \frac{\alpha}{\mu_i} \cdot (T_2 - T_1) \cdot \mu_e$$

$$\frac{L_2 - L_1}{L_1} = \frac{\mu_{i2} - \mu_{i1}}{\mu_{i2} \cdot \mu_{i1}} \mu_e$$

6.7 Temperature dependence of saturation magnetization

The saturation magnetization B_S drops monotonically with temperature and at T_C has fallen to $B_S = 0$ mT. The drop for $B_S(25\text{ °C})$ and $B_S(100\text{ °C})$, i.e. the main area of application for the ferrites, can be taken from the table of material properties.

6.8 Temperature dependence of saturation-dependent permeability (amplitude permeability)

It can be seen from the $\mu_a(B)$ curves for the different materials that μ_a exhibits a more pronounced maximum with increasing temperature and drops off sooner on account of decreasing saturation.

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7 Disaccommodation

Ferrimagnetic states of equilibrium can be influenced by mechanical, thermal or magnetic changes (shocks). Generally, an increase in permeability occurs when a greater mobility of individual magnetic domains is attained through the external application of energy. This state is not temporally stable and returns logarithmically with time to the original state.

7.1 Disaccommodation coefficient d

$$d = \frac{\mu_{i1} - \mu_{i2}}{\mu_{i1} \cdot (\lg t_2 - \lg t_1)}$$

μ_{i1} Permeability at time t_1

μ_{i2} Permeability at time t_2 and $t_2 > t_1$

7.2 Disaccommodation factor DF

$$DF = \frac{d}{\mu_{i1}}$$

Accordingly, a change in inductance can be calculated with the aid of DF :

$$\frac{L_1 - L_2}{L_1} = DF \cdot \mu_e \cdot \log \frac{t_2}{t_1}$$

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8 General mechanical, thermal, electrical and magnetic properties of ferrites

Typical figures for the mechanical and thermal properties of ferrites

Tensile strength	approx. 30 N/mm ²
Compressive strength	approx. 800 N/mm ²
Vickers hardness HV ₁₅	approx. 600 N/mm ²
Modulus of elasticity	approx. 150000 N/mm ²
Fracture toughness K _{1c}	approx. 0.8 ... 1.1 MPa·m ^{1/2}
Thermal conductivity	approx. 4 ... 7·10 ⁻³ J/mm·s·K
Coefficient of linear expansion	approx. 7 ... 10·10 ⁻⁶ 1/K
Specific heat	approx. 0.7 J/g·K

8.1 Mechanical properties

Ferrite cores have to meet mechanical requirements during assembling and for a growing number of applications. Since ferrites are ceramic materials one has to be aware of the special behavior under mechanical load.

As valid for any ceramic material, ferrite cores are brittle and sensitive to any shock, fast changing or tensile load. Especially high cooling rates under ultrasonic cleaning and high static or cyclic loads can cause cracks or failure of the ferrite cores.

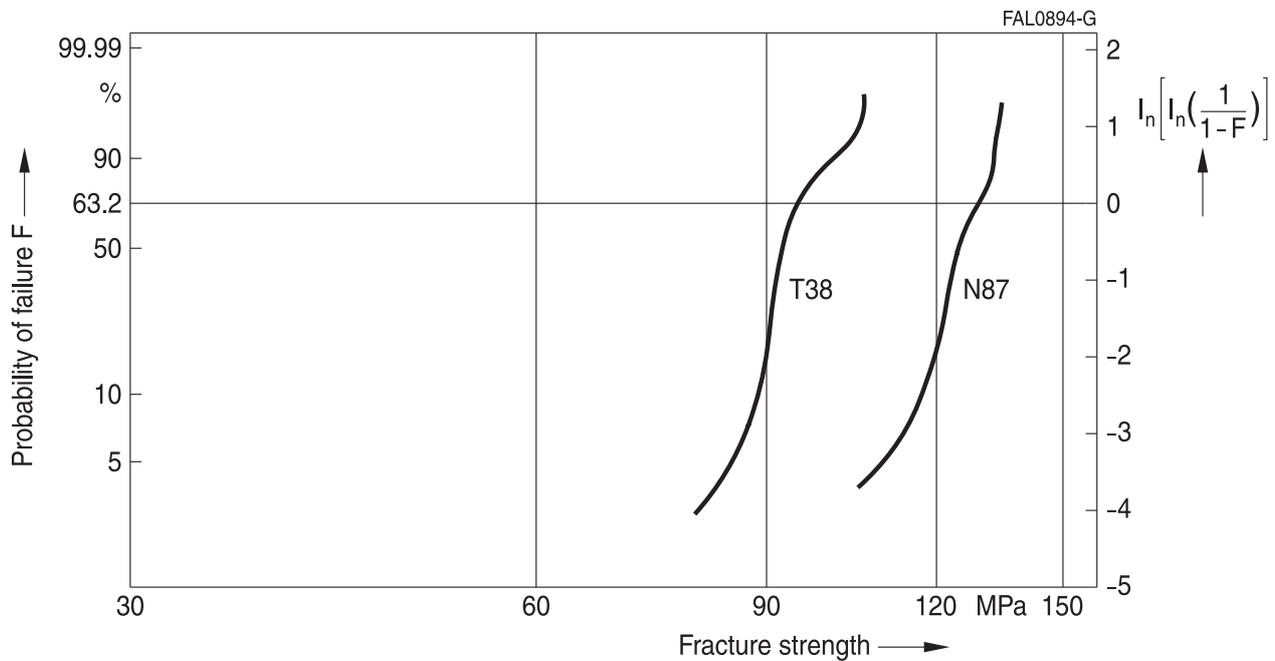


Figure 8 Weibull plot of fracture strength values of the materials T38 and N87

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There are two modes of crack growth: fast (critical) or slow (subcritical) crack propagation. In the first case spontaneous breakdown occurs. In the second case the crack propagates slowly during static or cycling loading, and then the sample can only fail if a critical crack length is achieved. According to the linear elastic fracture mechanics these two mechanisms could be described in terms of stress intensity factors. For life time predictions the knowledge of subcritical crack growth and R- (respectively K_{R-}) curve behavior of the material is essential.

The reduction of the material strength by temperature induced propagating microstructural cracks can be described as follows:

$$\sigma = \alpha \cdot \Delta T \frac{E_0}{1 + 2\pi N l^2}$$

σ	Effective strength
α	Coefficient of thermal expansion (7 to $12 \cdot 10^{-6}$ 1/K)
E_0	Modulus of elasticity
N	Number of temperature changes
l	Crack length

The brittleness of ferrite materials can be quantified by means of the fracture toughness. High fracture toughness values indicate decreased material brittleness. The quantity of the fracture toughness is a measure for the stress in the core necessary for a propagating crack. For the crack propagation it is required that the stress intensity factor exceeds the fracture toughness.

$$K_1 \geq K_{1C} \quad \text{with} \quad K_1 = \sigma_{\text{appl}} \sqrt{l \cdot Y} \quad \text{and} \quad K_{1C} = \sqrt{G_C E}$$

K_1	Stress intensity factor
K_{1C}	Fracture toughness
σ_{appl}	Applied stress
Y	Factor for fracture/sample geometry
G_C	Critical fracture area energy
E	Modulus of elasticity

Typical fracture toughness values are approx. 0.8 to 1.1 MPa·m^{1/2}.

Ferrite materials have a pronounced R curve behavior, i. e. the fracture toughness increases with propagating crack length. In practice there is a rather tolerant behavior towards moderate single stress events.

8.2 Stress sensitivity of magnetic properties

Stresses in the core affect not only the mechanical but also the magnetic properties. It is apparent that the initial permeability is dependent on the stress state of the core. With

$$\mu_i \cong \frac{1}{\frac{1}{\mu_{i0}} + k \cdot \sigma_T}; \quad k \approx 30 \cdot 10^{-6} \cdot \frac{1}{\text{MPa}}$$

where μ_{i0} is the initial permeability of the unstressed material, it can be shown that the higher the stresses are in the core, the lower is the value for the initial permeability. Embedding the ferrite cores (e.g. in plastic) can induce these stresses. A permeability reduction of up to 50% and more can be observed, depending on the material. In this case, the embedding medium should have the greatest possible elasticity.

8.3 Magnetostriction

Linear magnetostriction is defined as the relative change in length of a magnetic core under the influence of a magnetic field. The greatest relative variation in length $\lambda = \Delta l/l$ occurs at saturation magnetization. The values of the saturation magnetostriction (λ_s) of our ferrite materials are given in the following table (negative values denote contraction).

SIFERRIT material	K1	N48
λ_s in 10^{-6}	-18	-1.5

Magnetostrictive effects are of significance principally when a coil is operated in the frequency range <20 kHz and then undesired audible frequency effects (distortion etc.) occur.

8.4 Resistance to radiation

SIFERRIT materials can be exposed to the following radiation without significant variation ($\Delta L/L \leq 1\%$ for ungapped cores):

gamma quanta:	10^9 rad
quick neutrons	$2 \cdot 10^{20}$ neutrons/m ²
thermal neutrons	$2 \cdot 10^{22}$ neutrons/m ²

General

Definitions

8.5 Resistivity ρ , dielectric constant ϵ

At room temperature, ferrites have a resistivity in the range 1 Ωm to 10⁵ Ωm ; this value is usually higher at the grain boundaries than in the grain interior. The temperature dependence of the core resistivity corresponds to that of a semiconductor:

$$\rho \sim e^{\frac{E_a}{k \cdot T}}$$

- E_a Activation energy (0.1 to 0.5 eV)
- k Boltzmann constant
- T Absolute temperature (K)

Thus the resistivity at 100 °C is one order of magnitude less than at 25 °C, which is significant, particularly in power applications, for the magnitude of the eddy-current losses.

Similarly, the resistivity decreases with increasing frequency.

Example: Material N48

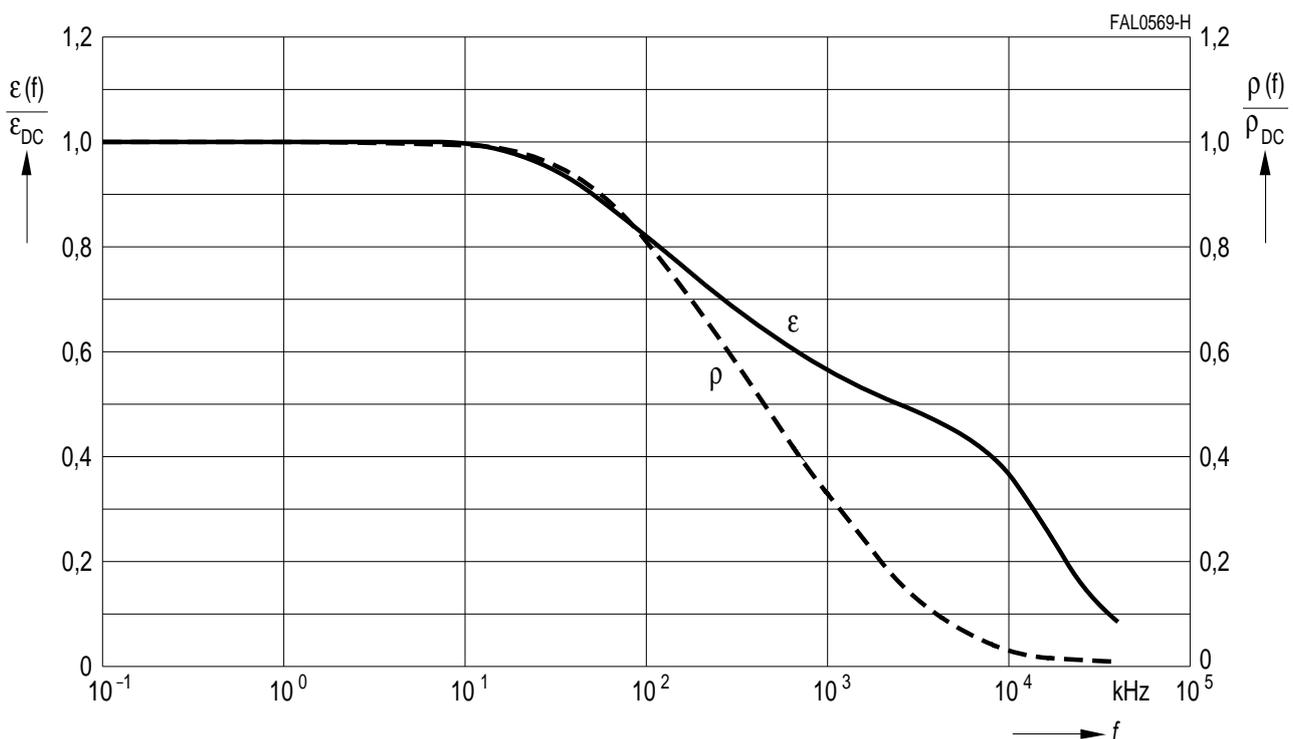


Figure 9
Resistivity and dielectric constant versus frequency

The different resistivity values for grain interior and grain boundary result in high (apparent) dielectric constants ϵ at low frequencies. The dielectric constant ϵ for all ferrites falls to values around 10 to 20 at very high frequencies. NiZn ferrites already reach this value range at frequencies around 100 kHz.

General

Definitions

SIFFERIT material	Resistivity (approx.) Ωm	Dielectric constant ϵ at (approximate values)				
		10 kHz	100 kHz	1 MHz	100 MHz	300 MHz
K1 (NiZn)	10^5	30	15	12	11	11
N48 (MnZn)	1	$140 \cdot 10^3$	$115 \cdot 10^3$	$80 \cdot 10^3$		

Magnetostrictive effects are of significance principally when a coil is operated in the frequency range <20 kHz and then undesired audible frequency effects occur.

9 Coil characteristics

Resistance factor A_R

The resistance factor A_R , or A_R value, is the DC resistance R_{Cu} per unit turn, analogous to the A_L value.

$$A_R = \frac{R_{Cu}}{N^2}$$

When the A_R value and number of turns N are given, the DC resistance can be calculated from $R_{Cu} = A_R N^2$.

From the winding data etc. the A_R value can be calculated as follows:

$$A_R = \frac{\rho \cdot l_N}{f_{Cu} \cdot A_N}$$

where ρ = resistivity (for copper: $17.2 \mu\Omega \text{ mm}$), l_N = average length of turn in mm, A_N = cross section of winding in mm^2 , f_{Cu} = copper space factor. If these units are used in the equation, the A_R value is obtained in $\mu\Omega = 10^{-6} \Omega$. For calculation of l_N and A_N the middle dimensions are used.

For coil formers, A_R values are given in addition to A_N and l_N . They are based on a copper filling factor of $f_{Cu} = 0.5$. This permits the A_R value to be calculated for any filling factor f_{Cu} :

$$A_{R(f_{Cu})} = A_{R(0.5)} \cdot \frac{0.5}{f_{Cu}}$$

For rough estimation a copper filling factor of $f_{Cu} = 0.5$ is sufficient.

Ferrites and accessories

Cautions and warnings

Mechanical stress and mounting

Ferrite cores have to meet mechanical requirements during assembling and for a growing number of applications. Since ferrites are ceramic materials one has to be aware of the special behavior under mechanical load.

As valid for any ceramic material, ferrite cores are brittle and sensitive to any shock, fast temperature changing or tensile load. Especially high cooling rates under ultrasonic cleaning and high static or cyclic loads can cause cracks or failure of the ferrite cores.

For detailed information see data book, chapter “*General - Definitions, 8.1*”.

Effects of core combination on A_L value

Stresses in the core affect not only the mechanical but also the magnetic properties. It is apparent that the initial permeability is dependent on the stress state of the core. The higher the stresses are in the core, the lower is the value for the initial permeability. Thus the embedding medium should have the greatest possible elasticity.

For detailed information see data book, chapter “*General - Definitions, 8.1*”.

Heating up

Ferrites can run hot during operation at higher flux densities and higher frequencies.

NiZn-materials

The magnetic properties of NiZn-materials can change irreversible in high magnetic fields.

Ferrite Accessories

Our ferrite accessories have been designed and evaluated only in combination with our ferrite cores. We explicitly point out that our ferrite accessories or our ferrite cores may not be compatible with those of other manufacturers. Any such combination requires prior testing by the customer and will be at the customer's own risk.

We assume no warranty or reliability for the combination of our ferrite accessories with cores and other accessories from any other manufacturer.

Processing remarks

The start of the winding process should be soft. Else the flanges may be destroyed.

- Too strong winding forces may blast the flanges or squeeze the tube that the cores can not be mounted any more.
- Too long soldering time at high temperature (>300 °C) may effect coplanarity or pin arrangement.
- Not following the processing notes for soldering of the J-leg terminals may cause solderability problems at the transformer because of pollution with Sn oxyde of the tin bath or burned insulation of the wire. For detailed information see chapter “*Processing notes*”, section 2.2.
- The dimensions of the hole arrangement have fixed values and should be understood as a recommendation for drilling the printed circuit board. For dimensioning the pins, the group of holes can only be seen under certain conditions, as they fit into the given hole arrangement. To avoid problems when mounting the transformer, the manufacturing tolerances for positioning the customers' drilling process must be considered by increasing the hole diameter.

Display of ordering codes for TDK Electronics products

The ordering code for one and the same product can be represented differently in data sheets, data books, other publications, on the company website or in order-related documents such as shipping notes, order confirmations and product labels. **The varying representations of the ordering codes are due to different processes employed and do not affect the specifications of the respective products.** Detailed information can be found on the Internet under www.tdk-electronics.tdk.com/orderingcodes.

Ferrites and accessories

Symbols and terms

Symbol	Meaning	Unit
A	Cross section of coil	mm ²
A _e	Effective magnetic cross section	mm ²
A _L	Inductance factor; $A_L = L/N^2$	nH
A _{L1}	Minimum inductance at defined high saturation ($\cong \mu_a$)	nH
A _{min}	Minimum core cross section	mm ²
A _N	Winding cross section	mm ²
A _R	Resistance factor; $A_R = R_{Cu}/N^2$	$\mu\Omega = 10^{-6} \Omega$
B	RMS value of magnetic flux density	Vs/m ² , mT
ΔB	Flux density deviation	Vs/m ² , mT
\hat{B}	Peak value of magnetic flux density	Vs/m ² , mT
$\Delta \hat{B}$	Peak value of flux density deviation	Vs/m ² , mT
B _{DC}	DC magnetic flux density	Vs/m ² , mT
B _R	Remanent flux density	Vs/m ² , mT
B _S	Saturation magnetization	Vs/m ² , mT
C ₀	Winding capacitance	F = As/V
CDF	Core distortion factor	mm ^{-4.5}
DF	Relative disaccommodation coefficient $DF = d/\mu_i$	
d	Disaccommodation coefficient	
E _a	Activation energy	J
f	Frequency	s ⁻¹ , Hz
f _{cutoff}	Cut-off frequency	s ⁻¹ , Hz
f _{max}	Upper frequency limit	s ⁻¹ , Hz
f _{min}	Lower frequency limit	s ⁻¹ , Hz
f _r	Resonance frequency	s ⁻¹ , Hz
f _{Cu}	Copper filling factor	
g	Air gap	mm
H	RMS value of magnetic field strength	A/m
\hat{H}	Peak value of magnetic field strength	A/m
H _{DC}	DC field strength	A/m
H _c	Coercive field strength	A/m
h	Hysteresis coefficient of material	10 ⁻⁶ cm/A
h/ μ_i^2	Relative hysteresis coefficient	10 ⁻⁶ cm/A
I	RMS value of current	A
I _{DC}	Direct current	A
\hat{I}	Peak value of current	A
J	Polarization	Vs/m ²
k	Boltzmann constant	J/K
k ₃	Third harmonic distortion	
k _{3c}	Circuit third harmonic distortion	
L	Inductance	H = Vs/A

Ferrites and accessories

Symbols and terms

Symbol	Meaning	Unit
$\Delta L/L$	Relative inductance change	H
L_0	Inductance of coil without core	H
L_H	Main inductance	H
L_p	Parallel inductance	H
L_{rev}	Reversible inductance	H
L_s	Series inductance	H
l_e	Effective magnetic path length	mm
l_N	Average length of turn	mm
N	Number of turns	
P_{Cu}	Copper (winding) losses	W
P_{trans}	Transferrable power	W
P_V	Relative core losses	mW/g
PF	Performance factor	
Q	Quality factor ($Q = \omega L/R_s = 1/\tan \delta_L$)	
R	Resistance	Ω
R_{Cu}	Copper (winding) resistance ($f = 0$)	Ω
R_h	Hysteresis loss resistance of a core	Ω
ΔR_h	R_h change	Ω
R_i	Internal resistance	Ω
R_p	Parallel loss resistance of a core	Ω
R_s	Series loss resistance of a core	Ω
R_{th}	Thermal resistance	K/W
R_V	Effective loss resistance of a core	Ω
s	Total air gap	mm
T	Temperature	$^{\circ}\text{C}$
ΔT	Temperature difference	K
T_C	Curie temperature	$^{\circ}\text{C}$
t	Time	s
t_v	Pulse duty factor	
$\tan \delta$	Loss factor	
$\tan \delta_L$	Loss factor of coil	
$\tan \delta_r$	(Residual) loss factor at $H \rightarrow 0$	
$\tan \delta_e$	Relative loss factor	
$\tan \delta_h$	Hysteresis loss factor	
$\tan \delta/\mu_i$	Relative loss factor of material at $H \rightarrow 0$	
U	RMS value of voltage	V
\hat{U}	Peak value of voltage	V
V_e	Effective magnetic volume	mm^3
Z	Complex impedance	Ω
Z_n	Normalized impedance $ Z _n = Z /N^2 \times \varepsilon (l_e/A_e)$	Ω/mm

Ferrites and accessories

Symbols and terms

Symbol	Meaning	Unit
α	Temperature coefficient (TK)	1/K
α_F	Relative temperature coefficient of material	1/K
α_e	Temperature coefficient of effective permeability	1/K
ϵ_r	Relative permittivity	
Φ	Magnetic flux	Vs
η	Efficiency of a transformer	
η_B	Hysteresis material constant	mT ⁻¹
η_i	Hysteresis core constant	A ⁻¹ H ^{-1/2}
λ_s	Magnetostriction at saturation magnetization	
μ	Relative complex permeability	
μ_0	Magnetic field constant	Vs/Am
μ_a	Relative amplitude permeability	
μ_{app}	Relative apparent permeability	
μ_e	Relative effective permeability	
μ_i	Relative initial permeability	
μ_p'	Relative real (inductive) component of $\bar{\mu}$ (for parallel components)	
μ_p''	Relative imaginary (loss) component of $\bar{\mu}$ (for parallel components)	
μ_r	Relative permeability	
μ_{rev}	Relative reversible permeability	
μ_s'	Relative real (inductive) component of $\bar{\mu}$ (for series components)	
μ_s''	Relative imaginary (loss) component of $\bar{\mu}$ (for series components)	
μ_{tot}	Relative total permeability derived from the static magnetization curve	
ρ	Resistivity	Ωm^{-1}
$\Sigma l/A$	Magnetic form factor	mm ⁻¹
τ_{Cu}	DC time constant $\tau_{Cu} = L/R_{Cu} = A_L/A_R$	s
ω	Angular frequency; $\omega = 2 \pi f$	s ⁻¹

All dimensions are given in mm.

SMD Surface-mount device

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The following applies to all products named in this publication:

1. Some parts of this publication contain **statements about the suitability of our products for certain areas of application**. These statements are based on our knowledge of typical requirements that are often placed on our products in the areas of application concerned. We nevertheless expressly point out **that such statements cannot be regarded as binding statements about the suitability of our products for a particular customer application**. As a rule, we are either unfamiliar with individual customer applications or less familiar with them than the customers themselves. For these reasons, it is always ultimately incumbent on the customer to check and decide whether a product with the properties described in the product specification is suitable for use in a particular customer application.
2. We also point out that **in individual cases, a malfunction of electronic components or failure before the end of their usual service life cannot be completely ruled out in the current state of the art, even if they are operated as specified**. In customer applications requiring a very high level of operational safety and especially in customer applications in which the malfunction or failure of an electronic component could endanger human life or health (e.g. in accident prevention or life-saving systems), it must therefore be ensured by means of suitable design of the customer application or other action taken by the customer (e.g. installation of protective circuitry or redundancy) that no injury or damage is sustained by third parties in the event of malfunction or failure of an electronic component.
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